

A Reconfigurable UWB Bandpass Filters with Embedded Multi-Mode Resonators

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How to cite this paper: Ouf, E.G., Mohra, A.S., Abdallah, E.A.-F. and Elhennawy, H. (2018) A Reconfigurable UWB Bandpass Filters with Embedded Multi-Mode Resonators. *Open Journal of Antennas and Propagation*, 6, 43-59.

<https://doi.org/10.4236/ojapr.2018.63005>

Received: August 16, 2018

Accepted: September 16, 2018

Published: September 19, 2018

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Abstract

The two proposed filters described here satisfy the Federal Communications Commission Ultra-wideband (FCC-UWB) specifications and also control the center frequency and bandwidth of the filters passband. These filters consist of two distinguishing parts, Electromagnetic bandgap (EBG)-embedded multiple-mode resonator (MMR) and interdigital coupled lines to realize high performance in the operation band with a compact size of 14.0 mm × 10.1 mm. The main advantage of the two proposed filters is that three different bands are tuned. The 1st tuned band is from 3.5 GHz to 11.4 GHz for the first filter and from 3.1 GHz to 11.6 GHz for the second proposed filter, respectively. The 2nd tuned band is from 3.5 GHz to 7.5 GHz for the first filter and from 3.1 GHz to 7.8 GHz for the second proposed filter, respectively. While the 3rd tuned band of the first proposed filter is from 3.5 GHz to 5.9 GHz and from 3.1 GHz to 5.8 GHz for the second proposed filter. The bandwidth of the filters can be changed by increasing the length of the outer open circuited stubs which are controlled by using switching matrix equipment (mini circuit, replacement of PIN diodes). To validate the design theory, a reconfigurable UWB bandpass filters (BPFs) with EBG Embedded MMR are designed, fabricated and measured. Good agreement is found between simulated and measured results.

Keywords

UWB Bandpass Filter, EBG, MMR, Reconfigurable, Stubs

1. Introduction

The filters play an important role in effectively transmitting the desired signals in certain passband regions while attenuating all the undesired signals in the re-

maintaining bandstop regions [1]. There are a lot of modern communication systems using the filters in their circuits, such as the embedded systems, mobile phone and wireless communication systems. It was necessary to explore alternative concepts because of the increasing demand for each of high-performance filters, circuit integration and reduced size [2]. The size of the filter can be reduced by reducing the resonator circuit with modifying its physical structures [3] [4]. Each of the conventional parallel coupled lines band-pass filter [5], U-shape resonators [6], open loops [7], and hairpin filters [8] helped in size reduction. The modern communication systems show a rapid evolution [9], that needs more size reduction of these resonators. The bandwidth and center frequency can be varied in tunable/reconfigurable band-pass filters.

Tunable bandwidth microwave filters are especially useful for the design of high-frequency multifunction receivers that support multiple information signals with different frequency bands.

Since that the UWB system has become one of the most favorable technologies for short-range low-power indoor wireless communications, and UWB BPF as one of the essential components of UWB systems (3.1 GHz - 10.6 GHz) has obtained much attention in recent years. The reconfigurable UWB bandpass filter (BPF) will be provided, whereas the recent advances in modern wideband radar and wireless communication applications need high performance, reconfigurable, and compact RF subsystems. Therefore, much attention has been devoted for compact reconfigurable microwave devices. An important component for the multifunction receivers is the UWB BPF with passband from 3.1 to 10.6 GHz. So far, various techniques have been recently developed for UWB bandpass filters. Since 2005, various UWB bandpass filters have been designed and reported, including filters of composite lowpass and highpass structure [10] [11], short-circuited stub filters [12] [13], and multiple-mode resonator (MMR) structure filters [14] [15].

In this paper, we present two Reconfigurable Ultra-Wideband Bandpass Filters with Embedded Multi-Mode Resonator and Electromagnetic Bandgap (MMR-EBG). The proposed UWB BPFs consist of two distinguishing parts, EBG-embedded MMR and interdigital coupled lines to realize high performance in the operation band with a compact size of 14.0 mm \times 10.1 mm. The MMR of the first proposed filter is formed by connected three open circuited stubs with two high impedance microstrip lines in center, but the MMR of the second proposed filter is formed by connected five open circuited stubs with four high impedance microstrip lines in center. The topology of a periodic structure with shunt capacitive loading is called electromagnetic bandgap (EBG) structures [16] [17]. The main advantage of the two proposed filters is introducing three different bands that can be tuned. The three different tuned bands for the first proposed filter are from 3.5 to 11.4 GHz, from 3.5 GHz to 7.5 GHz and from 3.5 GHz to 5.9 GHz, while the tuned bands for the second proposed filters are from 3.1 GHz to 11.6 GHz, from 3.1 GHz to 7.8 GHz and from 3.1 GHz to 5.8 GHz.

The reconfigurability of the proposed filters was proven by means of open and short circuits in certain locations which is controlled by using mini-circuit switching matrix equipment (which is the replacement of PIN diodes).

The paper is organized as follows: Section 2 provides the analysis of the proposed filter, and Section 3 introduces the design of the proposed filter in terms of the shape of the filter, its dimensions and the simulation results. Section 4 introduces the fabrication and the measurement of the proposed filters together with simulated results. The conclusion is given in Section 5.

2. Analysis of the Proposed Filter

Based on article [15], the corresponding equivalent circuit for the proposed filter is as shown in **Figure 1**. It is composed of MMR and J -inverters that represent the two coupled lines. The MMR is composed of EBG line in the center with two high impedance lines at two sides.

2.1. Analysis of the Input/Output Section

The input/output section is composed of two coupled lines with high impedance line as shown in **Figure 2**.

2.1.1. Analysis of the Two Coupled Line

The $ABCD$ matrix for the coupled line can be expressed as [18]:

$$M_c = \begin{bmatrix} \cos \theta_1 & jZ_o \sin \theta_1 \\ \frac{j \sin \theta_1}{Z_o} & \cos \theta_1 \end{bmatrix} \begin{bmatrix} 0 & -j \\ -jJ & 0 \end{bmatrix} \begin{bmatrix} \cos \theta_1 & jZ_o \sin \theta_1 \\ \frac{j \sin \theta_1}{Z_o} & \cos \theta_1 \end{bmatrix} \quad (1)$$

Z_o and θ_1 represent the characteristic impedance and the electrical length of the coupled line, respectively; while J is the admittance inverter. The admittance

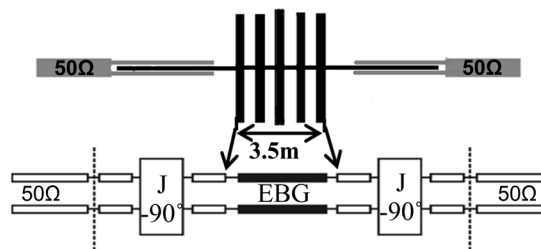


Figure 1. Schematic and equivalent transmission line network of the proposed UWB BPF on microstrip line topology [15].

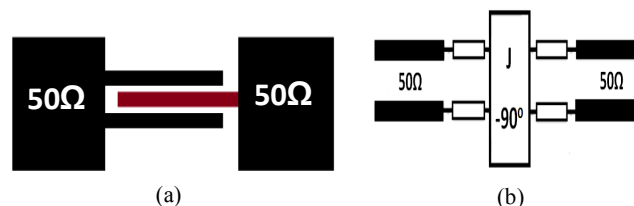


Figure 2. (a) Schematic and (b) equivalent transmission line network of the first part of the proposed filter.

inverter J in $ABCD$ matrix M_c can be replaced by the even and odd mode characteristic impedances (Z_{oe} & Z_{oo}) of the coupled line [18]:

$$JZ_o + \frac{1}{JZ_o} = \frac{Z_{oe} + Z_{oo}}{Z_{oe} - Z_{oo}} \tag{2}$$

$$JZ_o^2 = \frac{2}{Z_{oe} - Z_{oo}} \tag{3}$$

Substituting by Equation (2), and Equation (3) into Equation (1); the $ABCD$ matrix of the coupled line becomes:

$$M_c = \begin{bmatrix} \frac{Z_{oe} + Z_{oo}}{Z_{oe} - Z_{oo}} \cos \theta_1 & \frac{-j}{2} \left[\frac{4Z_{oe}Z_{oo}}{Z_{oe} - Z_{oo}} \frac{\cos^2 \theta_1}{\sin \theta_1} - (Z_{oe} - Z_{oo}) \sin \theta_1 \right] \\ j \frac{2}{Z_{oe} - Z_{oo}} \sin \theta_1 & \frac{Z_{oe} + Z_{oo}}{Z_{oe} - Z_{oo}} \cos \theta_1 \end{bmatrix} \tag{4}$$

Z_{oe} and Z_{oo} can be calculated as in [2].

2.1.2. High Impedance Line Analysis

The $ABCD$ matrix of the high impedance line can be expressed as [18]:

$$M_H = \begin{bmatrix} \cos \beta_H l_H & jZ_H \sin \beta_H l_H \\ \frac{j}{Z_H} \sin \beta_H l_H & \cos \beta_H l_H \end{bmatrix} \tag{5}$$

where Z_H is the highest line impedance, β_H is the propagation constant and l_H is the length of the high impedance line.

From Equation (4) & Equation (5), the $ABCD$ matrix of the first part of the proposed filter is:

$$M_1 = M_c \times M_H \tag{6}$$

Figure 3 shows the numerical results by using Mat-lab program version 2013 and simulated results by using CST MWS version 2014 of the input/output section. From **Figure 3**, it is clear that, both results are in good agreement.

2.2. Analysis of the Multi-Mode Resonator Section

The multi-mode resonator section can be considered as cascaded stepped impedance with high and low impedances as shown in **Figure 4**.

The $ABCD$ matrix of the second part can be expressed as follows [18]:

$$M_I = \begin{bmatrix} \cos \beta_1 l_1 & jZ_1 \sin \beta_1 l_1 \\ \frac{j}{Z_{c1}} \sin \beta_1 l_1 & \cos \beta_1 l_1 \end{bmatrix} \tag{7}$$

$$M_{II} = \begin{bmatrix} \cos \beta_2 l_2 & jZ_1 \sin \beta_2 l_2 \\ \frac{j}{Z_{c2}} \sin \beta_2 l_2 & \cos \beta_2 l_2 \end{bmatrix} \tag{8}$$

$$M_{III} = M_I \tag{9}$$

$$M_{IV} = M_{II} \tag{10}$$

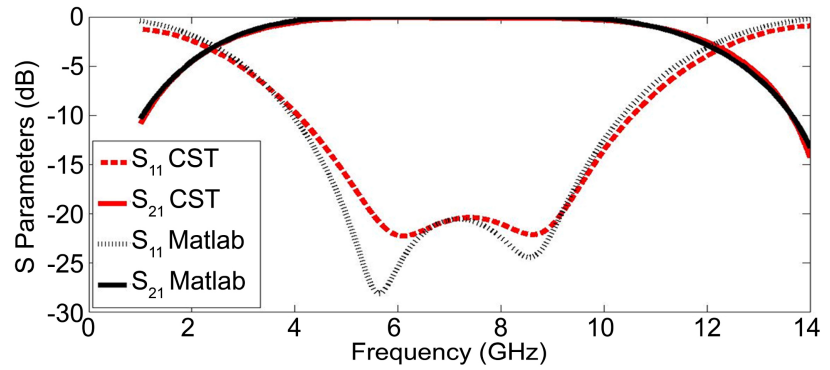


Figure 3. The numerical and simulated results for the input/output sections.

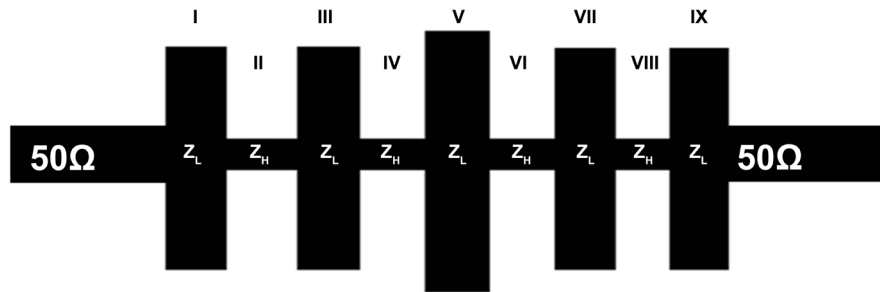


Figure 4. The multi-mode resonator section.

$$M_V = \begin{bmatrix} \cos \beta_5 l_5 & jZ_5 \sin \beta_5 l_5 \\ \frac{j}{Z_{c5}} \sin \beta_5 l_5 & \cos \beta_5 l_5 \end{bmatrix} \quad (11)$$

$$M_{VI} = M_{II} = M_{IV} \quad (12)$$

$$M_{VII} = M_{III} = M_I \quad (13)$$

$$M_{VIII} = M_{II} = M_{IV} = M_{VI} \quad (14)$$

$$M_{IX} = M_I = M_{III} = M_{VII} \quad (15)$$

From Equation (7) to Equation (15), the $ABCD$ matrix of the second part of the proposed filter is:

$$M_2 = M_I \times M_{II} \times \dots \times M_{IX} \quad (16)$$

The characteristic impedance and propagation constant of each section can be calculated as in [2].

Figure 5 shows the numerical results by using Mat-lab program version 2013 and simulated results by using CST MWS version 2014 of the Multi-mode resonator section. From Figure 5, it is clear that, both results are in good agreement.

Therefore, from the above discussion, it is clear that the total $ABCD$ matrix of the proposed filter can be expressed as:

$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = M_1 \times M_2 \times M_1 \quad (17)$$

The equations for computing the reflection and transmission coefficients from

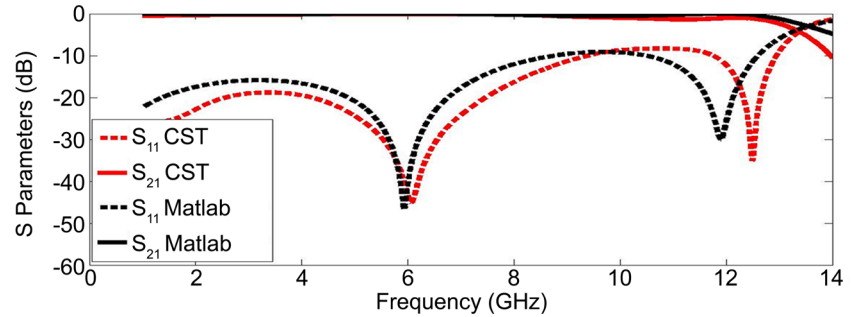


Figure 5. The numerical and simulated results for the Multi-mode resonator section.

the previous set of $ABCD$ -parameter values of the proposed filter can be written as follows [18]:

$$S_{11} = \frac{A + \frac{B}{Z_0} - cZ_0 - D}{A + \frac{B}{Z_0} + cZ_0 + D} \quad (18)$$

$$S_{21} = \frac{2}{A + \frac{B}{Z_0} + cZ_0 + D} \quad (19)$$

Figure 6 shows the numerical results by using Mat-lab program and simulated results by using CST MWS of the proposed filter. Regarding S_{11} , there is frequency shift about 0.6 GHz between the numerical and simulated results in the first resonant frequency. This may be attributed to the different method of analysis used in the CST and Mat-lab program, while this shift decreases with the second and third resonant frequency as illustrated in **Figure 6**. The S_{21} shows very good agreement between the simulated and the numerical results especially in the band of operation from 3.1 GHz to 11.6 GHz. Finally, from **Figure 6**, one can observe that both results are in good agreement.

3. Filter Design

The proposed filter is designed based on the example described in Ref. [19] but with a new contribution which is the controllable tunable bandwidth. This will be achieved by modifying the length of the outer open circuited stubs using diode switching matrix tools (instead of using PIN diodes). In this work, the proposed UWB-BPF consists of two parts, EBG-embedded MMR and interdigital coupled lines. The MMR is formed by connected series of open circuited stubs coupled with high impedance microstrip lines in center.

Three shapes of the proposed filter are presented, the first one is UWB BPF with MMR formed by three open circuited stubs mutually coupled with two high impedance microstrip lines in center, the second one is MMR formed by five open circuited stubs mutually coupled with four high impedance microstrip lines in center, and third one as same as the second one but with different length of each open circuited stubs.

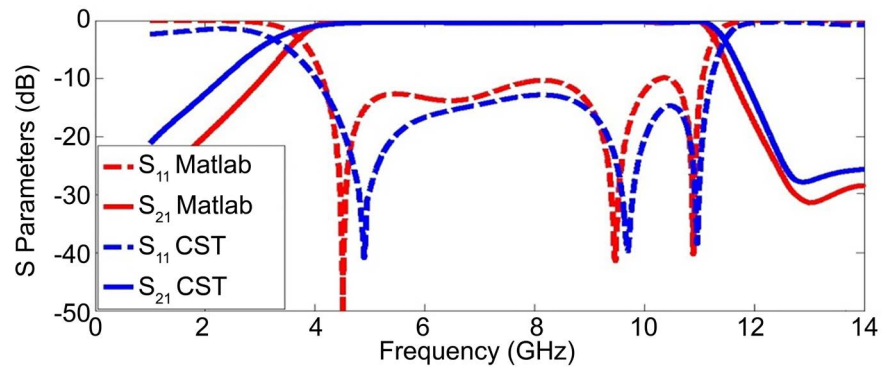


Figure 6. The numerical and simulated results of the proposed filter.

3.1. First Proposed Filter Design

The first proposed design with its optimized dimensions is shown in **Figure 7**. The overall dimension of the proposed filter is 14.0 mm × 10.1 mm. The filter operating bandwidth will be controlled by adjusting the length of the outer open circuited stubs (W_L). As W_L increases the bandwidth of the filter decreases as shown in **Table 1**. The length W_L is modified by using diodes switching matrix equipment where the character D refers to the diode and the different diodes states are described as follow:

1) When all the eight diodes ($D_1, D_2, D_3, D_4, D_5, D_6, D_7,$ and D_8) are in off state, the length W_L will be equal to 4.9 mm, so the bandwidth of the filter will be 7.9 GHz with band extends from 3.5 GHz to 11.4 GHz.

2) When $D_1, D_2, D_3,$ and D_4 are in on state; while $D_5, D_6, D_7,$ and D_8 are in off state, the length W_L will be equal to 7.5 mm, so the bandwidth of the filter will be 4 GHz with band extends from 3.5 GHz to 7.5 GHz.

3) When all diodes ($D_1, D_2, D_3, D_4, D_5, D_6, D_7,$ and D_8) are on, the length W_L will be equal to 10.1 mm, so the bandwidth of the filter will be 2.4 GHz with band extends from 3.5 GHz to 5.9 GHz.

From the above discussion, the length W_L can be modified to control the filter operating bandwidth. The above cases are summarized in **Table 1**.

Figure 8 shows the simulated results of the proposed filter with different lengths of the outer open circuited stubs (W_L) by using readymade software package (CST MWS version 2014). It is clear that the 3dB bandwidth of the bandpass filter varies according to W_L , and thus there are three tuned bands with the three different lengths (W_L).

3.2. The Second Proposed Filter Design

The second proposed design has five open circuited stubs mutually connected with four high impedance microstrip lines in middle as given in **Figure 9**. The overall dimension of the proposed filter is the same as the overall dimension of the first proposed filter (14.0 mm × 10.1 mm) and the design procedure of the second proposed filter is the same as in first shape, but the passband starts from 3.1 GHz instead of 3.5 GHz and so the bandwidth is changed also. These differences

Table 1. The S parameters against (W_L) for the first proposed filter.

W_L (mm)	-3 dB frequency band (GHz)	Minimum and maximum values of S parameters in passband (dB)		Roll off of passband and stop band (dB/GHz)	
		S_{11}	S_{21}	Pass band	Stop band
4.9	3.5 - 11.4	-3 to -45.4	-0.1 to -3	12.47	11.8
7.5	3.5 - 7.5	-3 to -63	-0.12 to -3	35.3	7.09
10.1	3.5 - 5.9	-3 to -42.6	-0.12 to -3	36.7	8.5

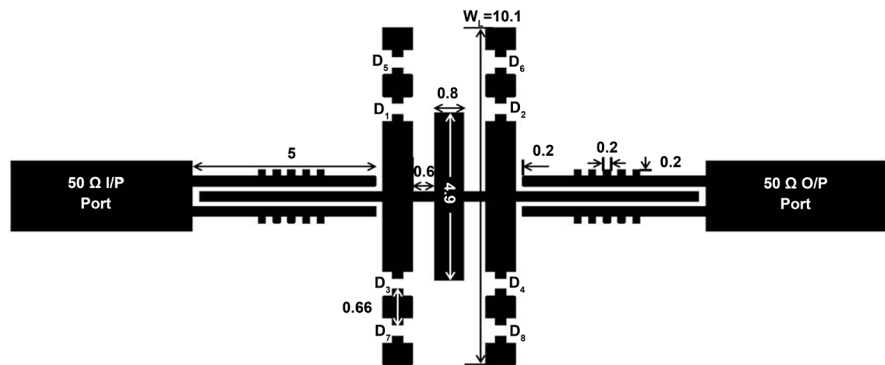


Figure 7. The proposed UWB BPF with three O.C. stubs and two high impedance microstrip lines (all dimensions in mm).

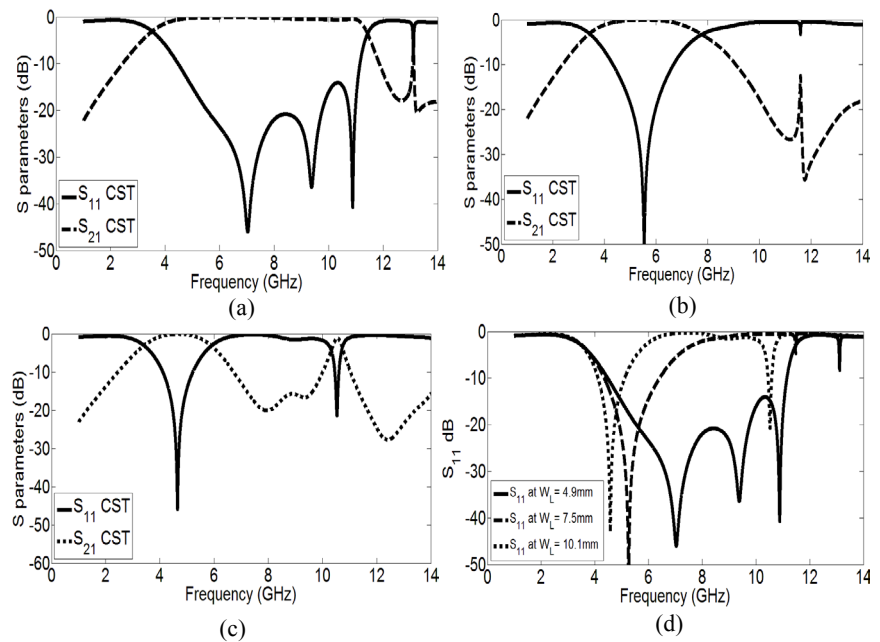


Figure 8. The simulated $|S_{11}|$ and $|S_{21}|$ using CST software package for different W_L lengths, (a) $W_L = 4.9$ mm; (b) $W_L = 7.5$ mm; (c) $W_L = 10.1$ mm; and (d) $|S_{11}|$ for all values of W_L .

are given in **Table 2.** **Figure 10** shows the simulated results of the second proposed filter design, there are three bands with different lengths of the outer open circuited stubs ($W_L = 4.9, 7.5, 10.1$ mm) by using CST. It should be noted that

Table 2. The S parameters against (W_L) for the second proposed filter.

W_L (mm)	-3 dB frequency band (GHz)	Minimum and maximum values of S parameters in passband (dB)		Roll off of passband and stop band (dB/GHz)	
		S_{11}	S_{21}	Pass band	Stop band
4.9	3.1 - 11.6	-3 to -47.3	-0.14 to -3	27.7	10.5
7.5	3.1 - 7.8	-3 to -39.8	-0.12 to -3	30.7	8.1
10.1	3.1 - 5.8	-3 to -36.5	-0.12 to -3	41.9	8.9

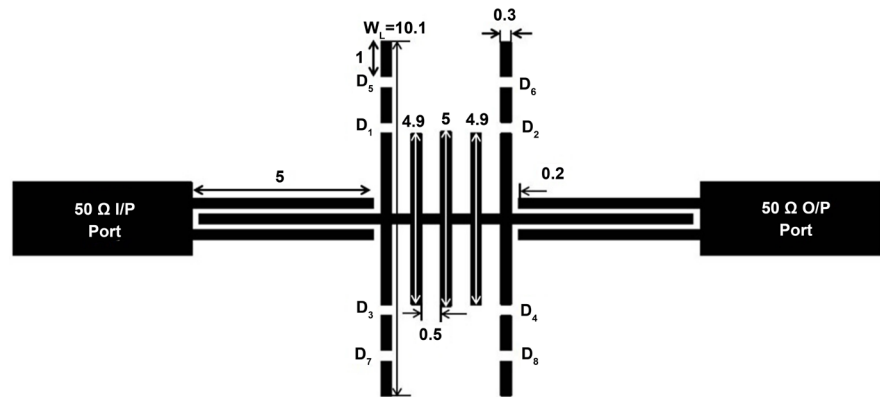


Figure 9. The proposed UWB BPF with five O.C. stubs and four high impedance microstrip lines (all dimensions in mm).

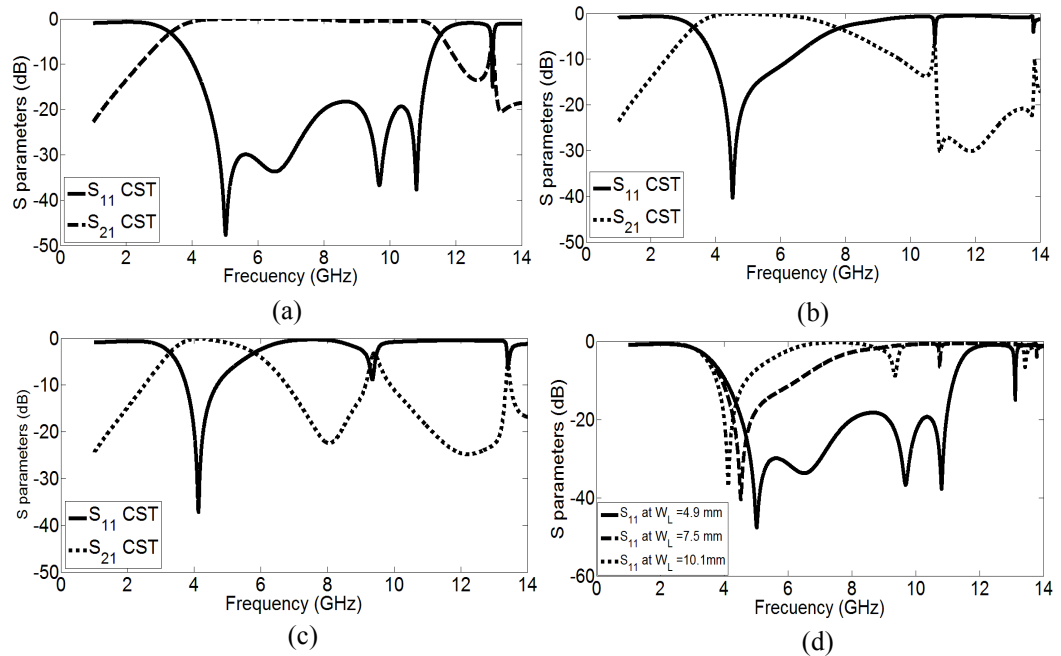


Figure 10. The simulated $|S_{11}|$ and $|S_{21}|$ using CST software package for different W_L lengths, (a) $W_L = 4.9$ mm; (b) $W_L = 7.5$ mm; (c) $W_L = 10.1$ mm; and (d) $|S_{11}|$ for all values of W_L .

the roll off of the second filter in the passband is better than the first one, and the bandwidth increased to 8.5 GHz instead of 7.9 GHz as shown in **Table 2**. Also the first resonance of the second filter occurs at 5 GHz instead of 6.9 GHz

for the first filter as in **Figure 11**, so the performance of the second filter is better than the first one especially for the case of $W_L = 4.9$ mm.

3.3. The Modification of the Second Proposed Filter

From the second proposed filter performance, it is noticed that the selectivity and the out of band rejection are bad, so it has been modified to improve them. An optimization procedure was carried out and the length L_3 was changed from 5 mm to 4 mm, L_2 changed from 4.9 mm to 3.6 mm, and L_1 remains the same as shown in **Figure 12**.

The design procedure of the modified filter is the same as in the second proposed filter. **Figure 13** shows the simulated results of the modified filter design, there are three bands with different lengths of the outer open circuited stubs ($W_L = 4.9, 7.5, 10.1$ mm) by using CST.

It should be noticed that the selectivity is improved and the out of band rejection has become better (S_{21} improved by more than 20 dB from 11.6 to 14 GHz) for the case of $W_L = 4.9$ mm as in **Figure 14**, and as in **Table 3**.

Our proposed designed filter is compared with similar filters as given in **Table 4**, where we noticed that the proposed filters are distinguished from the other published filters due to smaller size and larger bandwidth. The proposed design achieves total area reduction of more than 50% compared with [21], 70% compared with [22], and 54% compared with [23]. It also provides a wider operating bandwidth, achieving a 10.6% increase in bandwidth compared with [20] [23], 18.6% compared with [21], and 1.2% compared with [22].

4. Fabrication and Measurements

The designed filters are fabricated using thin film technology and photolithographic technique on Rogers RO3006 (lossy) substrate with ($\epsilon_r = 6.15$, $h = 1.52$ mm, and $\tan \delta = 0.002$). The photos for the fabricated filters are shown in **Figure 15**. The connecting wires are soldered to the circuit, and then connecting the diode switch matrix tool (that replaces the PIN diode switch). The filters are

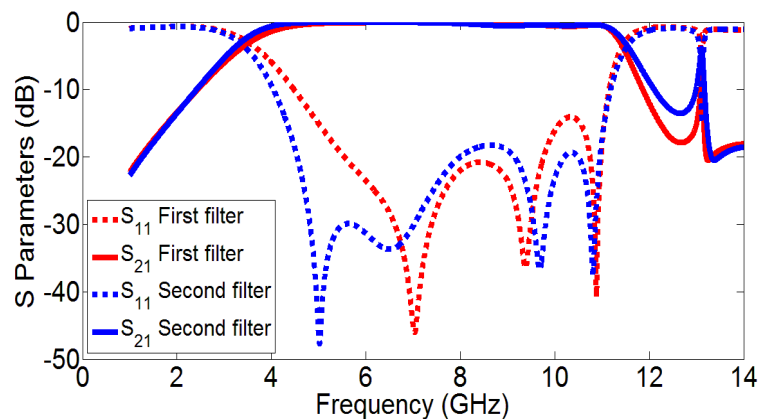


Figure 11. The simulated $|S_{11}|$ and $|S_{21}|$ using CST software package for the first and the second filters.

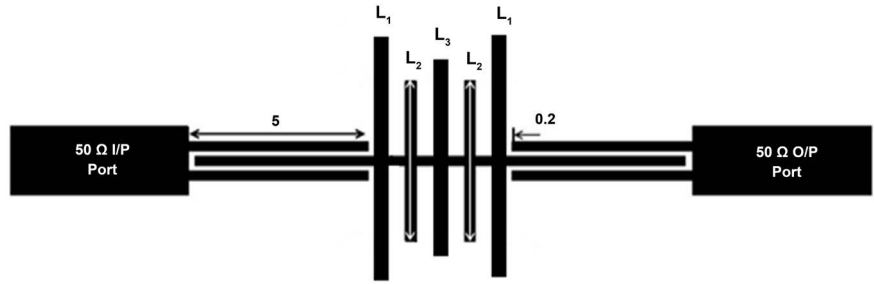


Figure 12. The modified UWB BPF with five O.C. stubs and four high impedance microstrip lines (all dimensions in mm).

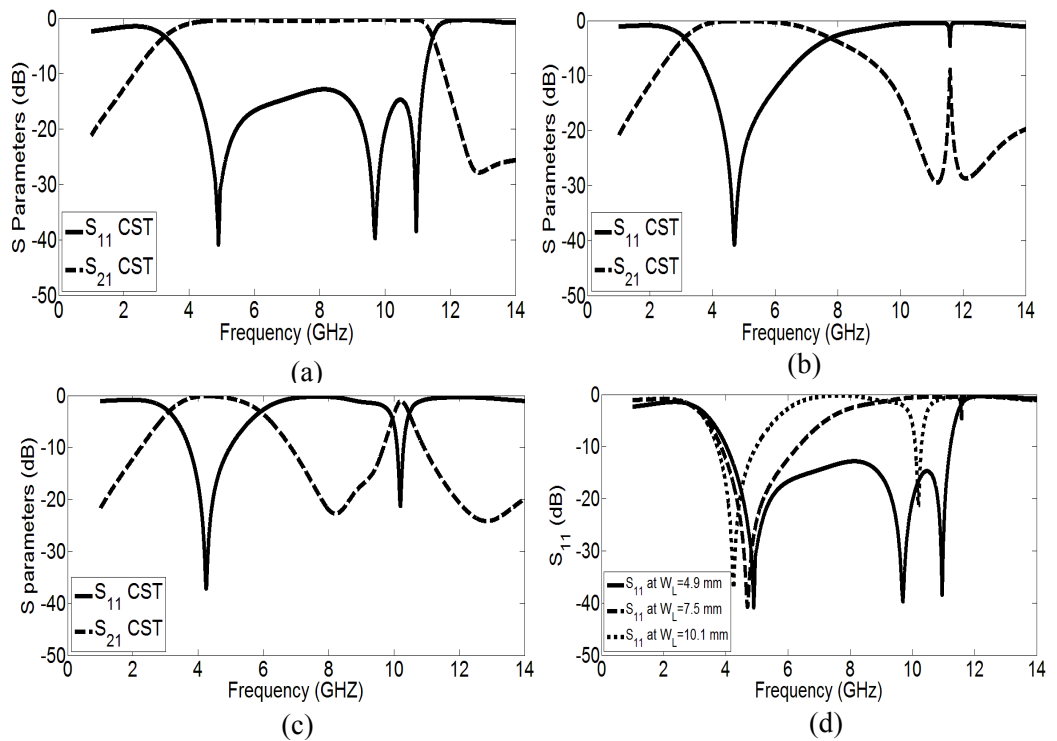


Figure 13. The simulated $|S_{11}|$ and $|S_{21}|$ for the modification of the second proposed filter design using CST software package for different W_L lengths. (a) $W_L = 4.9$ mm; (b) $W_L = 7.5$ mm; (c) $W_L = 10.1$ mm; and (d) $|S_{11}|$ for all W_L .

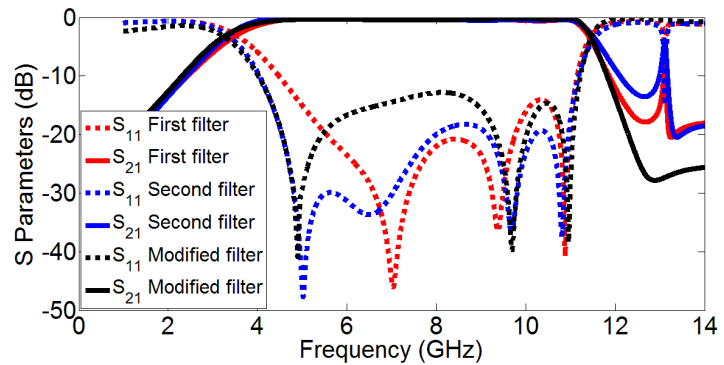


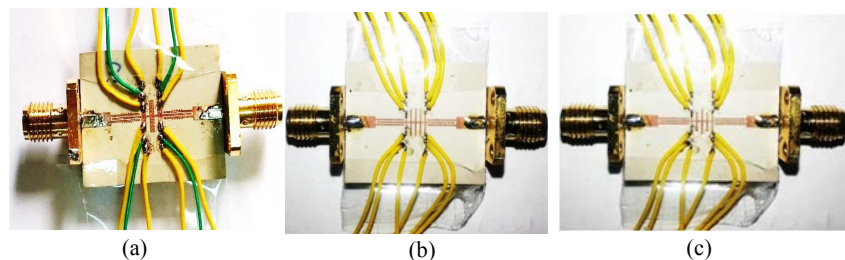
Figure 14. The simulated $|S_{11}|$ and $|S_{21}|$ using CST software package for the three shapes of filters.

Table 3. The S parameters against (W_L) for the modified proposed filter.

W_L (mm)	-3 dB frequency band (GHz)	Minimum and maximum values of S parameters in passband (GHz)		Roll off of passband and stop band (dB/GHz)	
		S_{11} (dB)	S_{21} (dB)	Pass band	Stop band
4.9	3.1 to 11.6	-3 to -43.5	-0.2 to -3	27.8	15.7
7.5	3.1 to 7.8	-3 to -39.2	-0.1 to -3	25.9	8.4
10.1	3.1 to 5.8	-3 to -36.8	-0.13 to -3	33.8	8.5

Table 4. Comparison of the proposed filter with published UWB Bandpass filters.

Ref.	Dielectric constant (ϵ_r)	Height (mm)	Size of filter	Center frequency f_0 (GHz)	Passband (GHz)
Ref. [20]	10.8	0.635	23.98 mm \times 4.96 mm	6.85	3.1 - 10.6
Ref. [21]	3.38	0.508	20 mm \times 15 mm	7.1	3.6 - 10.6
Ref. [22]	2.65	1	30 mm \times 16 mm	6.85	2.8 - 11.0
Ref. [23]	2.55	0.8	22.51 mm \times 13.66 mm	6.85	3.1 - 10.6
1st filter	6.15	1.52	14.0 mm \times 10.1 mm	7.45	3.5 - 11.4
Our work 2nd filter	6.15	1.52	14.0 mm \times 10.1 mm	7.35	3.1 - 11.6
modified	6.15	1.52	14.0 mm \times 10.1 mm	7.35	3.1 - 11.6

**Figure 15.** Photos for the fabricated filters, (a) First shape; (b) Second shape; (c) Third shape.

measured using the vector network analyzer (N9928A FieldFox Handheld Microwave Vector Network Analyzer, 26.5 GHz.).

Figures 16-18 show the measured and simulated results of the three structures. The measured results are consistent with the simulated ones. The measured 3dB passband of the first proposed filter is between 3.5 to 11.4 GHz in the 1st band, while in the second and third proposed filter is from 3.1 GHz to 11.6 GHz, from 3.5 to 7.5 GHz in the 2nd band of the first filter, while in the second and third filter from 3.1 GHz to 7.8 GHz, and from 3.5 to 5.9 GHz in the 3rd band of the first filter, while in the second and third filter from 3.1 GHz to 5.8 GHz. All filters have compact sizes with dimensions 14.0 mm \times 10.1 mm.

Figure 18(a) shows the measured and simulated $|S_{11}|$ and $|S_{21}|$ of the modified filter with five open circuit stubs with frequency range from 1 GHz to 20 GHz at $W_L = 4.9$ mm. It should be noted that the frequency range is extended up to 20

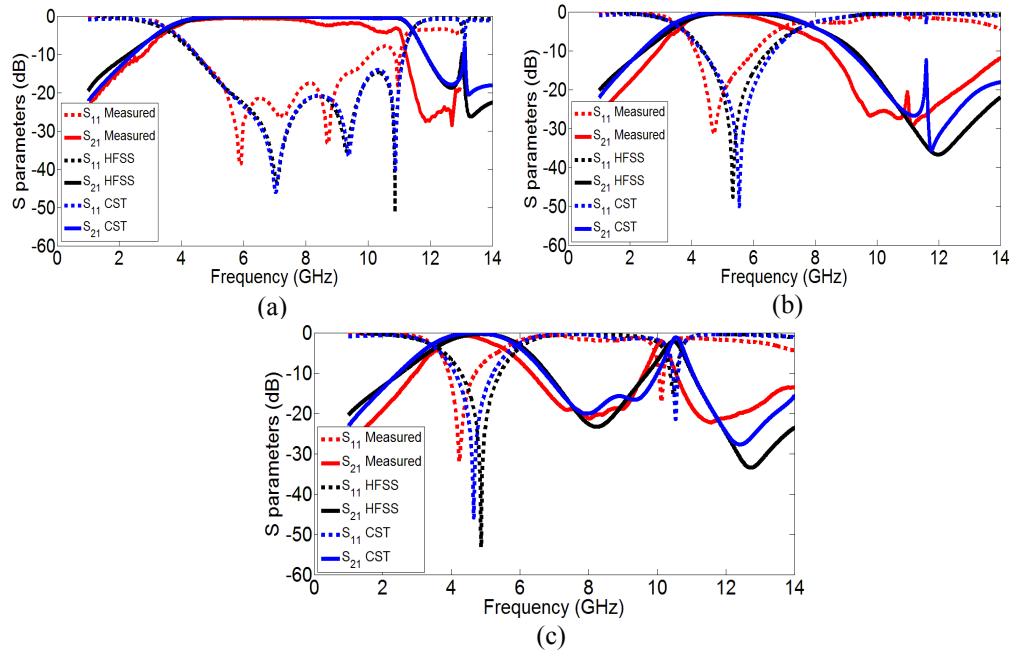


Figure 16. The simulated and measured $|S_{11}|$ and $|S_{21}|$ for the first filter shape for different W_L lengths (a) $W_L = 4.9$ mm; (b) $W_L = 7.5$ mm; and (c) $W_L = 10.1$ mm.

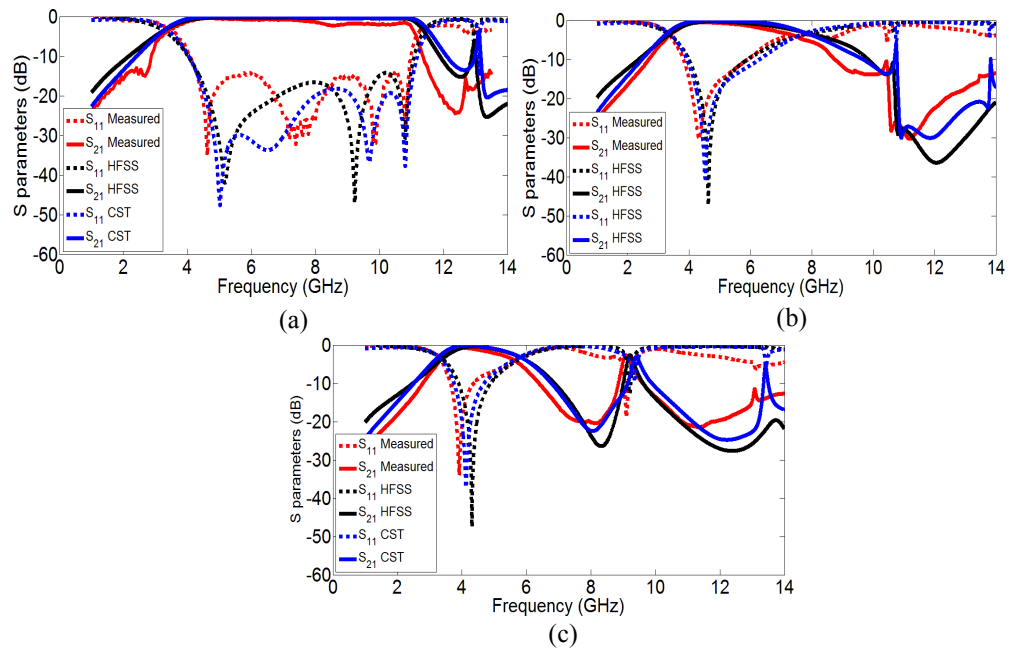


Figure 17. The simulated and measured $|S_{11}|$ and $|S_{21}|$ for the second filter shape for different W_L lengths (a) $W_L = 4.9$ mm; (b) $W_L = 7.5$ mm; and (c) $W_L = 10.1$ mm.

GHz in order to show that the out of band rejection has been improved due to the modifications that were carried out in the lengths of the open circuit stubs. HFSS software package was also used as another simulation tool to validate and verify the obtained performance of the proposed filters. **Figure 19** shows the group delay variations for the three shapes of the proposed filters simulated by

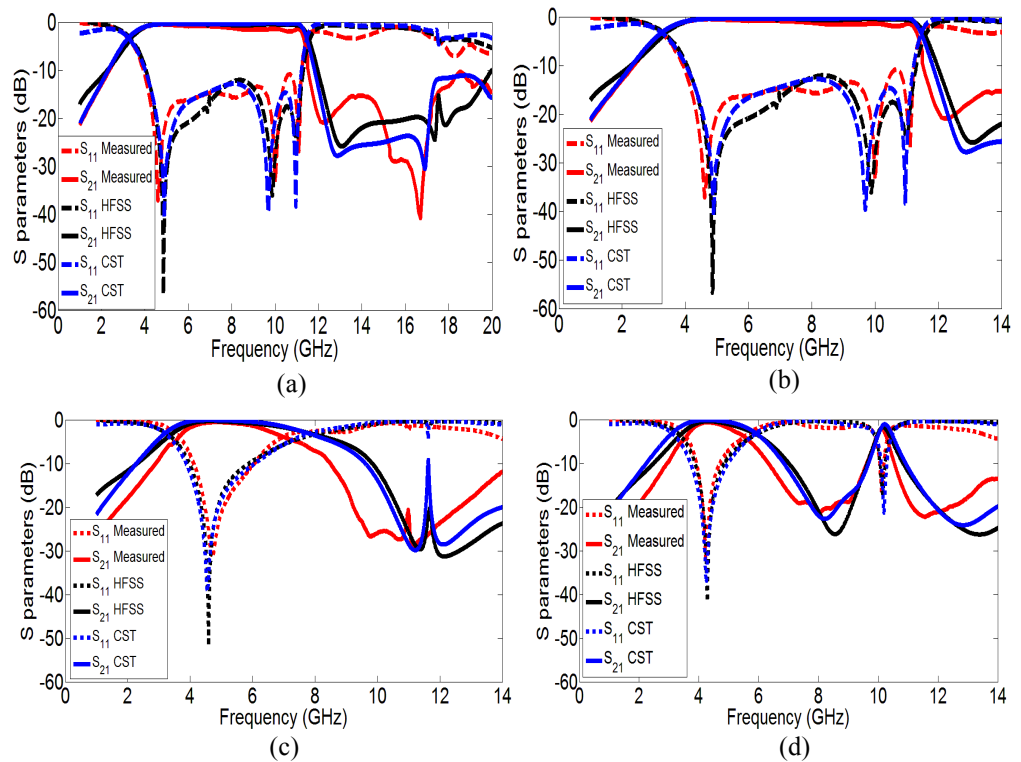


Figure 18. The simulated and measured $|S_{11}|$ and $|S_{21}|$ for the modification of the second proposed filter for different W_L lengths (a) $W_L = 4.9$ mm (with frequency range from 1 GHz to 20 GHz); (b) $W_L = 4.9$ mm; (c) $W_L = 7.5$ mm and (d) $W_L = 10.1$ mm.

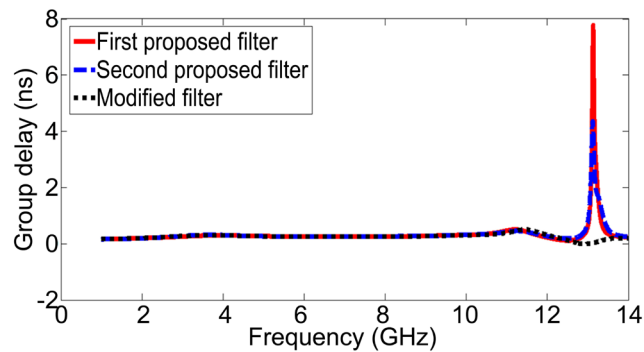


Figure 19. The group delay for the three shapes of the proposed filter.

the CST MWS software. It should be noted that the maximum variation of group delay within 1 - 14 GHz is 0.4 ns for the modified filter, while the maximum variation of group delay for second proposed filter is 4.35 ns, and for the first proposed filter is 7.68 ns. As can be noted that the reported values for the modified proposed filter is lower than the other two proposed filters and indicates a very low distortion that can be happened for the modified filter.

From the above figures, one can notice that:

- 1) There is a difference between the first, second, and third shape of the proposed filter in the frequency band and the center frequency as shown in **Table 5**, as well as differences in group delay and roll off behavior.

Table 5. Comparison between the three shapes of the proposed filters.

No. of filter shape at $W_L = 4.9$ mm	-3 dB frequency band (GHz)	Minimum and maximum values of S parameters in passband (GHz)		Roll off of passband and stop band (dB/GHz)		Impedance matching (dB)	Group delay at (1 - 14 GHz) (ns)
		S_{11} (dB)	S_{21} (dB)	Pass band	Stop band		
Shape 1	3.5 to 11.4	-3 to -45.4	-0.1 to -3	12.47	11.8	<-15	0.15 - 7.68
Shape 2	3.1 to 11.6	-3 to -47.3	-0.14 to -3	27.7	10.5	<-20	0.15 - 4.35
Shape 3	3.1 to 11.6	-3 to -43.5	-0.2 to -3	27.8	15.7	<-15	0.15 - 0.4

2) The insertion loss within the pass band of the two shapes is the same.

3) The fabrication of the second and third shapes is more difficult than the first shape.

4) The slope of the insertion loss of the third shape is sharper than the first and second shape.

5. Conclusion

Reconfigurable Ultra-Wideband Bandpass Filters with EBG Embedded Multi-Mode Resonator have been designed, simulated, and fabricated. Two packages of software were used, namely CST MWS 2014 and 3D EM commercial software HFSS version 13.0 to design and simulate the filters. The simulated and measured results are comparable. The measured results were characterized using a N9928A FieldFox Handheld Microwave Vector Network Analyzer, 26.5 GHz. Small size and three different frequency bands add some advantages to these filters. By adjusting the length of the outer open circuit stubs, the center frequency and the 3 dB frequency band can be easily adjusted. The final size of these filters is 14.0 mm \times 10.1 mm, which is suitable for modern ultra-wide band wireless communication systems. According to The FCC regulations, the proposed filters in all their structures satisfy the definitions of the UWB filters whether according to the first definition of FCC which is 3.1 - 10.6 GHz bandwidth requirements or according the second definition which is 500 MHz bandwidth requirements. So, the proposed filter can be used in communication systems with UWB application [24].

Conflicts of Interest

The authors declare no conflicts of interest regarding the publication of this paper.

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